

1 TITLE OF THE INVENTION

MICROPHONE ARRAY APPARATUS

BACKGROUND THE INVENTION

5 1. Field of the Invention

The present invention relates to a microphone array apparatus which has an array of microphones in order to detect the position of a sound source, emphasize a target sound and suppress noise.

10 The microphone array apparatus has an array of a plurality of omnidirectional microphones and equivalently define a directivity by emphasizing a target sound and suppressing noise. Further, the microphone array apparatus is capable of detecting the position of a sound source on the basis of a relationship among the phases of output signals of the microphones. Hence, the microphone array apparatus can be applied to a video conference system in which a video camera is automatically oriented towards a speaker and a speech signal and a video signal can concurrently be transmitted. In addition, the speech of the speaker can be clarified by suppressing ambient noise. The speech of the speaker can be emphasized by adding the phases of speech components. It is now required that the microphone array apparatus can stably operate.

25 If the microphone array apparatus is directed to suppressing noise, filters are connected to respective microphones and filter coefficients are adaptively or fixedly set so as to minimize noise components (see, for example, Japanese Laid-Open Patent Application No. 5-111090). If the microphone array apparatus is directed to detecting the position of a sound source, the relationship among the phases of the output signals of the microphones is detected, and the distance to the sound source is detected (see, for example, Japanese Laid-Open Patent Application

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1 Nos. 63-177087 and 4-236385).

2 An echo canceller is known as a device which
3 utilizes the noise suppressing technique. For
4 example, as shown in Fig. 1, a transmit/receive
5 interface 202 of a telephone set is connected to a
6 network 203. An echo canceller is connected between a
7 microphone 204 and a speaker 205. A speech of a
8 speaker is input to the microphone 204. A speech of a
9 speaker on the other (remote) side is reproduced
10 through the speaker 205. Hence, a mutual
11 communication can take place.

12 A speech transferred from the speaker 205 to
13 the microphone 204, as indicated by a dotted line
14 shown in Fig. 1 forms an echo (noise) to the other-
15 side telephone set. Hence, the echo canceller 201 is
16 provided that includes a subtracter 206, an echo
17 component generator 207 and a coefficient calculator
18 208. Generally, the echo generator 207 has a filter
19 structure which produces an echo component from the
20 signal which drives the speaker 205. The subtracter
21 206 subtracts the echo component from the signal from
22 the microphone 204. The coefficient calculator 208
23 controls the echo generator 207 to update the filter
24 coefficients so that the residual signal from the
25 subtracter 206 is minimized.

26 The updating of the filter coefficients c_1 ,
27 c_2 , ..., c_r of the echo component generator 207 having
28 the filter structure can be obtained by a known
29 maximum drop method. For example, the following
30 evaluation function J is defined based on an output
31 signal e (the residual signal in which the echo
32 component has been subtracted) of the subtracter 206:

$$J = e^2 \quad (1)$$

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36 According to the above evaluation function, the filter
37 coefficients c_1 , c_2 , ..., c_r are updated as follows:

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$$\begin{aligned} 1 \quad & \begin{bmatrix} c1 \\ c2 \\ . \\ . \\ cr \end{bmatrix} = \begin{bmatrix} c1_{old} \\ c2_{old} \\ . \\ . \\ cr_{old} \end{bmatrix} + \alpha * (e / f_{norm}) * \begin{bmatrix} f(1) \\ f(2) \\ . \\ . \\ f(r) \end{bmatrix} \\ 5 \quad & \end{aligned} \quad (2)$$

where $0.0 < \alpha < 0.5$

$$10 \quad f_{norm} = (f(1)^2 + f(2)^2 + \dots + f(r)^2)^{1/2} \quad (3)$$

In the above expressions, a symbol "*" denotes multiplication, and "r" denotes the filter order. Further, $f(1)$, ..., $f(r)$ respectively denote the values of a memory (delay unit) of the filter (in other words, the output signals of delay units each of which delays the respective input signal by a sample unit). A symbol " f_{norm} " is defined as equation (3), and a symbol " α " is a constant, which represents the speed and precision of convergence of the filter coefficients towards the optimal values.

The echo canceller 201 has filter orders as many as 100. Hence, another echo canceller using a microphone array as shown in Fig. 2 is known. There are provided an echo canceller 211, a transmit/receive interface 212, microphones 214-1 - 214-n forming a microphone array, a speaker 215, a subtracter 216, filters 217-1 - 217-n, and a filter coefficient calculator 218.

In the structure shown in Fig. 2, acoustic components from the speaker 215 to the microphones 214-1 - 214-n are propagated along routes indicated by broken lines and serve as echoes. Hence, the speaker 215 is a noise source. The updating control of the filter coefficients $c11$, $c12$, ..., clr , ..., $cn1$, $cn2$, ..., cnr in the case where the speaker does not make any speech is expressed by using the evaluation function (1) as follows:

$$\begin{bmatrix} c11 \\ c12 \\ \vdots \\ clr \end{bmatrix} = \begin{bmatrix} c11_{old} \\ c12_{old} \\ \vdots \\ clr_{old} \end{bmatrix} - \alpha * (e / f_{lnorm}) * \begin{bmatrix} fl(1) \\ fl(2) \\ \vdots \\ fl(r) \end{bmatrix} \quad \dots (4)$$

$$\begin{bmatrix} cp1 \\ cp2 \\ \vdots \\ cpr \end{bmatrix} = \begin{bmatrix} cp1_{old} \\ cp2_{old} \\ \vdots \\ cpr_{old} \end{bmatrix} + \alpha * (e / f_{pnorm}) * \begin{bmatrix} fp(1) \\ fp(2) \\ \vdots \\ fp(r) \end{bmatrix} \quad (5)$$

where $p = 2, 3, \dots, n$

The equation (4) relates to a case where one of the microphones 214-1 - 214-n, for example, the microphone 214-1 is defined as a reference microphone, and indicates the filter coefficients $c11, c12, \dots, clr$ of the filter 217-1 which receives the output signal of the above reference microphone 214-1. The equation (5) relates to the microphones 214-2 - 214-n other than the reference microphones, and indicates the filter coefficients $c21, c22, \dots, c2r, \dots, cn1, cn2, \dots, cnr$. The subtracter 216 subtracts the output signals 217-2 - 217-n of the microphones 214-2 - 214-n from the output signal 217-1 of the reference microphone 214-1.

Fig. 3 is a block diagram for explaining a conventional process of detecting the position of a sound source and emphasizing a target sound. The structure shown in Fig. 3 includes a target sound emphasizing unit 221, a sound source detecting unit 222, delay units 223 and 224, a number-of-delayed-samples calculator 225, an adder 226, a crosscorrelation coefficient calculator 227, a position detection processing unit 228 and microphones 229-1 and 229-2.

The target sound emphasizing unit 221

1 includes the delay units 223 and 224 of z^{-da} and z^{-db} ,
the number-of-delayed-samples calculator 225 and the
adder 226. The sound source position detecting unit
222 includes the crosscorrelation coefficient
5 calculator 227 and the position detection processing
unit 228. The number-of-delayed samples calculator
225 is controlled by the following factors. The
crosscorrelation coefficient calculator 227 of the
sound source position detecting unit 222 obtains a
10 crosscorrelation coefficient $r(i)$ of output signals
 $a(j)$ and $b(j)$ of the microphones 229-1 and 229-2. The
position detection processing unit 228 obtains the
sound source position by referring to a value of i ,
 i_{max} , at which the maximum of the crosscorrelation
15 coefficient $r(i)$ can be obtained.

The crosscorrelation coefficient $r(i)$ is
expressed as follows:

$$r(i) = \sum_{j=1}^n a(j) * b(j+i) \quad (6)$$

20 where $\sum_{j=1}^n$ denotes a summation of $j=1$ to $j=n$, and i
has a relationship $-m \leq i \leq m$. The symbol " m " is a
value dependent on the distance between the
microphones 229-1 and 229-2 and the sampling
25 frequency, and is written as follows:

$$m = [(\text{sampling frequency}) * (\text{intermicrophone distance})] / (\text{speed of sound}) \quad (7)$$

30 where n is the number of samples for a convolutional
operation.

The number of delayed samples da of the z^{-da}
delay unit 223 and the number of delayed samples db of
the z^{-db} delay unit 224 can be obtained as follows
35 from the value i_{max} at which the maximum value of the
crosscorrelation coefficient $r(i)$ can be obtained:

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1 where $i \geq 0$, $da = i$, $db = 0$
 where $i < 0$, $da = 0$, $db = -i$.

5 Hence, the phases of the target sound from the sound
 source are made to coincide with each other and are
 added by the adder 226. Hence, the target sound can
 be emphasized.

 However, the above-mentioned conventional
 microphone array apparatus has the following
10 disadvantages.

 In the conventional structure directed to
 suppressing noise, when the speaker of the target
 sound source does not speak, the echo components from
 the speaker to the microphone array can be canceled by
15 the echo canceller. However, when a speech of the
 speaker and the reproduced sound from the speaker are
 concurrently input to the microphone array, the
 updating of the filter coefficients for canceling the
 echo components (noise components) does not converge.
20 That is, the residual signal e in the equations (4)
 and (5) corresponds to the sum of the components which
 cannot be suppressed by the subtracter 216 and the
 speech of the speaker. Hence, if the filter
 coefficients are updated so that the residual signal e
25 is minimized, the speech of the speaker which is the
 target sound is suppressed along with the echo
 components (noise). Hence, the target noise cannot be
 suppressed.

 In the conventional structure directed to
30 detecting the sound source position and emphasizing
 the target sound, the output signals $a(j)$ and $b(j)$ of
 the microphones 229-1 and 229-2 shown in Fig. 3
 generally have an autocorrelation in the vicinity of
 the sampled values. If the sound source is white
35 noise or pulse noise, the autocorrelation is reduced,
 while the autocorrelation for vice is increased. The
 crosscorrelation function $r(i)$ defined in the equation

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- 1 (6) has a less variation as a function of i with
respect to a signal having comparatively large
autocorrelation than a variation with respect to a
signal having comparatively small autocorrelation.
5 Hence, it is very difficult to obtain the correct
maximum value and precisely and rapidly detect the
position of the sound source.

- In the conventional structure directed to
emphasizing the target sound so that the phases of the
10 target sounds are synchronized, the degree of emphasis
depends on the number of microphones forming the
microphone array. If there is a small
crosscorrelation between the target sound and noise,
the use of N microphones emphasizes the target sound
15 so that the power ratio is as large as N times. If
there is a large correction between the target sound
and noise, the power ratio is small. Hence, in order
to emphasize the target sound which has a large
crosscorrelation to the noise, it is required to use a
20 large number of microphones. This leads to an
increase in the size of the microphone array. It is
very difficult to identify, under noisy environment,
the position of the power source by utilizing the
crosscorrelation coefficient value of the equation
25 (6).

SUMMARY OF THE INVENTION

- It is a general object of the present
invention to provide a microphone array apparatus in
30 which the above disadvantages are eliminated.

- A more specific object of the present
invention is to provide a microphone array apparatus
capable of stably and precisely suppressing noise,
emphasizing a target sound and identifying the
35 position of a sound source.

The above objects of the present invention
are achieved by a microphone array apparatus

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1 comprising: a microphone array including microphones
(which correspond to parts indicated by reference
numbers 1-1 - 1-n in the following description), one
of the microphones being a reference microphone (1-1);
5 filters (2-1 - 2-n) receiving output signals of the
microphones; and a filter coefficient calculator (4)
which receives the output signals of the microphones,
a noise and a residual signal obtained by subtracting
10 filtered output signals of the microphones other than
the reference microphone from a filtered output signal
of the reference microphone and which obtain filter
coefficients of the filters in accordance with an
evaluation function based on the residual signal.
With this structure, even when speech of a speaker
15 corresponding to the sound source and the noise are
concurrently applied to the microphones, the
crosscorrelation function value is reduced so that the
noise can be effectively suppressed and the filter
coefficients can continuously be updated.

20 The above microphone array apparatus may be
configured so that it further comprises: delay units
(8-1 - 8-n) provided in front of the filters; and a
delay calculator (9) which calculates amounts of
delays of the delay units on the basis of a maximum
25 value of a crosscorrelation function of the output
signals of the microphones and the noise. Hence, the
filter coefficients can easily be updated.

The microphone array apparatus may be
30 configured so that the noise is a signal which drives
a speaker. This structure is suitable for a system
that has a speaker in addition to the microphones. A
reproduced sound from the speaker may serve as noise.
By handling the speaker as a noise source, the signal
driving the speaker can be handled as the noise, and
35 thus the filter coefficients can easily be updated.

The microphone array apparatus may further
comprise a supplementary microphone (21) which outputs

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1 the noise. This structure is suitable for a system
which has microphones but does not have a speaker.
The output signal of the supplementary microphone can
be used as the noise.

5 The microphone array apparatus may be
configured so that the filter coefficient calculator
includes a cyclic type low-pass filter (Fig. 10) which
applies a comparatively small weight to memory values
of a filter portion which executes a convolutional
10 operation in an updating process of the filter
coefficients.

The above objects of the present invention
are also achieved by a microphone array apparatus
comprising: a microphone array including microphones
15 (51-1, 51-2); linear predictive filters (52-1, 52-2)
receiving output signals of the microphones; linear
predictive analysis units (53-1, 53-2) which receives
the output signals of the microphones and update
filter coefficients of the linear predictive filters
20 in accordance with a linear predictive analysis; and a
sound source position detector (54) which obtains a
crosscorrelation coefficient value based on linear
predictive residuals of the linear predictive filters
and outputs information concerning the position of a
25 sound source based on a value which maximizes the
crosscorrelation coefficient. Hence, even when speech
of a speaker corresponding to the sound source and the
noise are concurrently applied to the microphones,
autocorrelation function values of samples about the
30 speech signal are reduced to the linear predictive
analysis, so that the position of the target source
can accurately be detected. Thus, speech from the
target sound can be emphasized and noise components
other than the target sound can be suppressed.

35 The microphone array apparatus may be
configured so that: a target sound source is a
speaker; and the linear predictive analysis unit

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1 updates the filter coefficients of the linear
predictive filters by using a signal which drives the
speaker. Hence, the linear predictive analysis unit
can be commonly used to the linear predictive filters
5 corresponding to the microphones.

The above-mentioned objects of the present
invention are achieved by a microphone array apparatus
comprising: a microphone array including microphones
(61-1, 61-2); a signal estimator (62) which estimates
10 positions of estimated microphones in accordance with
intervals at which the microphones are arranged by
using the output signals of the microphones and a
velocity of sound and which outputs output signals of
the estimated microphones together with the output
15 signals of the microphones forming the microphone
array; and a synchronous adder (63) which pulls phases
of the output signals of the microphones and the
estimated microphones and then adds the output
signals. Hence, even if a small number of microphones
20 is used to form an array, the target sound can be
emphasized and the position of the target sound source
can precisely be detected as if a large number of
microphones is used.

The microphone array apparatus may further
25 comprise a reference microphone (71) located on an
imaginary line connecting the microphones forming the
microphone array and arranged at intervals at which
the microphones forming the microphone array are
arranged, wherein the signal estimator which corrects
30 the estimated positions of the estimated microphones
and the output signals thereof on the basis of the
output signals of the microphones forming the
microphone array.

The microphone array apparatus may further
35 comprise an estimation coefficient decision unit (74)
weights an error signal which corresponds to a
difference between the output signal of the reference

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1 microphone and the output signals of the signal
estimator in accordance with an acoustic sense
characteristic so that the signal estimator performs a
signal estimating operation on a band having a
5 comparatively high acoustic sense with a comparatively
high precision.

The microphone array apparatus may be
configured so that: given angles are defined which
indicate directions of a sound source with respect to
10 the microphones forming the microphone array; the
signal estimator includes parts which are respectively
provided to the given angles; the synchronous adder
includes parts which are respectively provided to the
given angles; and the microphone array apparatus
15 further comprises a sound source position detector
which outputs information concerning the position of a
sound source based on a maximum value among the output
signals of the parts of the synchronous adder.

The above objects of the present invention
20 are also achieved by a microphone array apparatus
comprising: a microphone array including microphones
(91-1, 91-2); a sound source position detector (92)
which detects a position of a sound source on the
basis of output signals of the microphones; a camera
25 (90) generating an image of the sound source; a second
detector (93) which detects the position of the sound
source on the basis of the image from the camera; and
a joint decision processing unit (94) which outputs
information indicating the position of the sound
30 source on the basis of the information from the sound
source position detector and the information from the
second detector. Hence, the position of the target
sound source can be rapidly and precisely detected.

35 BRIEF DESCRIPTION OF THE DRAWINGS

Other objects, features and advantages of
the present invention will become more apparent from

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1 the following detailed description when read in
conjunction with the accompanying drawings, in which:

Fig. 1 is a block diagram of a conventional
echo canceller;

5 Fig. 2 is a diagram of a conventional echo
canceller using a microphone array;

Fig. 3 is a block diagram of a structure
directed to detecting the position of a sound source
and emphasizing the target sound;

10 Fig. 4 is a block diagram of a first
embodiment of the present invention;

Fig. 5 is a block diagram of a filter which
can be used in the first embodiment of the present
invention;

15 Fig. 6 is a block diagram of a second
embodiment of the present invention;

Fig. 7 is a flowchart of an operation of a
delay calculator used in the second embodiment of the
present invention;

20 Fig. 8 is a block diagram of a third
embodiment of the present invention;

Fig. 9 is a block diagram of a fourth
embodiment of the present invention;

25 Fig. 10 is a block diagram of a low-pass
filter used in a filter coefficient updating process
executed in the embodiments of the present invention;

Fig. 11 is a block diagram of a structure
using a digital signal processor (DSP);

30 Fig. 12 is a block diagram of an internal
structure of the DSP shown in Fig. 11;

Fig. 13 is a block diagram of a delay unit;

Fig. 14 is a block diagram of a fifth
embodiment of the present invention;

35 Fig. 15 is a block diagram of a detailed
structure of the fifth embodiment of the present
invention;

Fig. 16 is a diagram showing a relationship

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1 between the sound source position and $imax$;

Fig. 17 is a block diagram of a sixth embodiment of the present invention;

5 Fig. 18 is a block diagram of a seventh embodiment of the present invention;

Fig. 19 is a block diagram of a detailed structure of the seventh embodiment of the present invention;

10 Fig. 20 is a block diagram of an eighth embodiment of the present invention;

Fig. 21 is a block diagram of a ninth embodiment of the present invention; and

Fig. 22 is a block diagram of a tenth embodiment of the present invention.

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DESCRIPTION OF THE PREFERRED EMBODIMENTS

A description will now be given, with reference to Fig. 4, of a microphone array apparatus according to a first embodiment of the present invention. The apparatus shown in Fig. 4 is made up of n microphones 1-1 - 1- n forming a microphone array, filters 2-1 - 2- n , an adder 3, a filter coefficient calculator 4, a speaker (target sound source) 5, and a speaker (noise source). The speech of the speaker 5 is input to the microphones 1-1 - 1- n , which converts the received acoustic signals into electric signals, which pass through the filters 2-1 - 2- n and are then applied to the adder 3. The output signal of the adder 3 is then to a remote terminal via a network or the like. A speech signal from the remote side is applied to the speaker 6, which is thus driven to reproduce the original speech. Hence, the speaker 5 communicates with the other-side speaker. The reproduced speech is input to the microphones 1-1 - 1- n , and thus functions as noise to the speech of the speaker 5. Hence, the speaker 6 is a noise source with respect to the target sound source.

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1 The filter coefficient calculator 4 is
supplied with the output signals of the microphones 1-
1 - 1-n, a noise (an input signal for driving the
speaker serving as noise source), and the output
5 signal (residual signal) of the adder 3, and thus
updates the coefficients of the filters 2-1 - 2-n. In
this case, the microphone 1-1 is handled as a
reference microphone. The subtracter 3 subtracts the
output signals of the filters 2-2 - 2-n from the
10 output signal of the filter 2-1.

Each of the filters 2-1 - 2-n can be
configured as shown in Fig. 5. Each filter includes
 z^{-1} delay units 11-1 - 11-r-1, coefficient units 12-1.
- 12-r for multiplication of filter coefficients cp1,
15 cp2, ..., cpr, and adders 13 and 14. A symbol "r"
denotes the order of the filter.

When the signal from the noise source
(speaker 6) is denoted as xp(i) and the signal from
the target sound source (speaker 5) is denoted as
20 yp(i) (where i denotes the sample number and p is
equal to 1, 2, ..., n), the values fp(i) of the
memories of the filters 2-1 - 2-n (the input signals
to the filters and the output signals of the delay
units 11-1 - 11-r-1) are defined as follows:

$$25 \quad \quad \quad fp(i) = xp(i) + yp(i) \quad (8)$$

The output signal e of the adder in the echo
canceller using the conventional microphone array is
30 as follows:

$$e = [f_1(1) \cdot \cdot \cdot f_1(r)] \begin{bmatrix} c_{11} \\ c_{12} \\ \vdots \\ c_{1r} \end{bmatrix}$$

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$$- \sum_{i=2}^n [f_i(1) \cdot \cdot \cdot f_i(r)] \begin{bmatrix} c_{i1} \\ c_{i2} \\ \vdots \\ c_{ir} \end{bmatrix} \quad \dots (9)$$

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1 where $f_1(1), f_1(2), \dots, f_1(r), \dots, f_i(1),$
 $f_i(2), \dots, f_i(r)$ denote the values of the memories of
the filters. The adder subtracts the output signals
of the filters other than the reference filter from
5 the output signal of the reference filter.

In contrast, the present invention controls
the signals $x_p(i)$ in phase and performs the
convolutional operation. The output signal e' of the
adder thus obtained is as follows:

$$\begin{aligned}
 10 \quad e' &= [f_1(1)' \cdots f_1(r)'] \begin{bmatrix} c_{11} \\ c_{12} \\ \vdots \\ c_{1r} \end{bmatrix} \\
 &\quad - \sum_{i=2}^n [f_i(1)' \cdots f_i(r)'] \begin{bmatrix} c_{i1} \\ c_{i2} \\ \vdots \\ c_{ir} \end{bmatrix} \quad \dots (10) \\
 &\quad [f_p(1)' \cdots f_p(r)'] \\
 20 \quad &= [x(1)(p) \cdots x(q)(p)] \begin{bmatrix} f_p(1) \cdots f_p(r) \\ f_p(2) \cdots f_p(r+1) \\ \vdots \\ f_p(q) \cdots f_p(q+r-1) \end{bmatrix} \\
 &\quad \dots (11)
 \end{aligned}$$

25 where (p) in $x(1)(p), \dots, x(q)(p)$ denotes signals
from the noise source obtained when the microphones 1-
1 - 1-n are in phase, and the symbol "q" denotes the
number of samples on which the convolutional operation
is executed.

30 When the signals $x_p(i)$ from the noise source
and the signals $y_p(i)$ of the target sound source are
concurrently input, that is, when the speaker 5 speaks
at the same time as the speaker 6 outputs a reproduced
speech, there is a small crosscorrelation therebetween
because the coexisting speeches are uttered by
35 different speakers. Hence, the equation (11) can be
rewritten as follows:

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$$\begin{aligned}
 & [fp(1)' \cdot \cdot \cdot fp(r)'] \\
 & = [x(1)(p) \cdot \cdot \cdot x(q)(p)] \begin{bmatrix} fp(1) \cdot \cdot \cdot fp(r) \\ fp(2) \cdot \cdot \cdot fp(r+1) \\ \vdots \\ fp(q) \cdot \cdot \cdot fp(q+r-1) \end{bmatrix} \\
 5 & \\
 & = [x(1)(p) \cdot \cdot \cdot x(q)(p)] \begin{bmatrix} \{xp(1)+yp(1)\} \cdots \{xp(r)+yp(r)\} \\ \{xp(2)+yp(2)\} \cdots \{xp(r+1)+yp(r+1)\} \\ \vdots \\ \{xp(q)+yp(q)\} \cdots \{xp(q+r-1)+yp(q+r-1)\} \end{bmatrix} \\
 10 & \\
 & \doteq \left[\sum_{i=1}^q x(i)(p) * xp(i) \cdot \cdot \cdot \sum_{i=1}^q x(i)(q) * xp(r+i-1) \right] \cdots (12)
 \end{aligned}$$

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It can be seen from the above equation (12), an influence of the signals $yp(i)$ from the target sound source to $[fp(1)', \dots, fp(r)']$ is reduced. The signal e' in the equation (10) is obtained by using the equation (12), and then, an evaluation function $J = (e')^2$ is calculated based on the obtained signal e' . Then, based on the evaluation function $J = (e')^2$, the filter coefficients of the filters 2-1 - 2-n are updated. That is, even in the state in which speeches from the speaker (target sound source) 5 and the speaker (noise source) 6 are concurrently applied to the microphones 1-1 - 1-n, the noise contained in the output signals of the microphones 1-1 - 1-n has a large crosscorrelation to the input signal applied to the filter coefficient calculator 4 and used to drive the speaker 6, while having a small crosscorrelation to the target sound source 5. Hence, the filter coefficients can be updated in accordance with the evaluation function $J = (e')^2$. Hence, the output signal of the adder 3 is the speech signal of the speaker 5 in which the noise is suppressed.

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Fig. 6 is a block diagram of a microphone array apparatus according to a second embodiment of

1 the present invention in which parts that are the same
as those shown in the previously described figures are
given the same reference numbers. The structure shown
in Fig. 6 includes delay units 8-1 - 8-n ($z^{-d_1} - z^{-d_n}$),
5 and a delay calculator 9.

The updating of the filter coefficients according to the second embodiment of the present invention is based on the following. The delay calculator 9 calculates the number of delayed samples
10 in each of the delay units 8-1 - 8-n so that the output signals of the microphones 1-1 - 1-n are pulled in phase. Further, the filter coefficient calculator 4 calculates the filter coefficients of the filters 2-1 - 2-n. The delay calculator 9 is supplied with the
15 output signals of the microphones 1-1 - 1-n, and the input signal (noise) for driving the speaker 6. The filter coefficient calculator 4 is supplied with the output signals of the delay units 8-1 - 8-n, the output signal of the adder 3 and the input signal
20 (noise) for driving the speaker 6.

When the output signals of the microphones 1-1 - 1-n are denoted as $gp(i)$ where $p = 1, 2, \dots, n$; j is the sample number, a crosscorrelation function $Rp(i)$ to the signals $x(j)$ from the noise source is as
25 follows:

$$Rp(i) = \sum_{j=1}^s gp(j+i) * x(j) \quad (13)$$

where $\sum_{j=1}^s$ denotes a summation from $j=1$ to $j=s$, and s
30 denotes the number of samples on which the convolutional operation is executed. The number s of samples may be equal to tens to hundreds of samples. When a symbol "D" denotes the maximum delayed sample corresponding to the distances between the noise
35 source and the microphones, the term "i" in the equation (13) is such that $i = 0, 1, 2, \dots, D$.

For example, when the maximum distance

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1 between the noise source and the furthest microphone
is equal to 50 cm, and the sampling frequency is equal
to 8 kHz, the speed of sound is approximately equal to
340 m/s, and thus the maximum number D of delayed
5 samples is as follows:

$$\begin{aligned} D &= (\text{sampling frequency}) * (\text{maximum distance} \\ &\quad \text{between the noise source and} \\ &\quad \text{microphone}) / (\text{speed of sound}) \\ 10 \quad &= 8000 * (50 / 34000) = 11.76 \approx 12. \end{aligned}$$

Hence, the symbol "i" is equal to 1, 2, ..., 12. When
the maximum distance between the noise source and the
microphone is equal to 1m, the maximum number D of
15 delayed samples is equal to 24.

The value i_p ($p = 1, 2, \dots, n$) is obtained
which is the value of i obtained when the absolute
value of the crosscorrelation function value $R_p(i)$
obtained by equation (13). Further, the maximum value
20 i_{\max} of the i_p is obtained. The above process is
comprised of steps (A1) - (A11) shown in Fig. 7. The
term i_{\max} is set to an initial value (equal to, for
example, 0) and the variable p is set equal to 1, at
step A1. At step A2, the term $R_{p\max}$ is set to an
25 initial value (equal to, for example, 0.0), and the
term i_p is set to an initial value (equal to, for
example, 0). Further, at step A2, the variable i is
set equal to 0. At step A3, the crosscorrelation
function value $R_p(i)$ defined by the equation (13) is
30 obtained.

At step A4, it is determined whether the
crosscorrelation function value $R_p(i)$ is greater than
the term $R_{p\max}$. If the answer is YES, the $R_p(i)$
obtained at that time is set to $R_{p\max}$ at step A5. If
35 the answer is NO, the variable i is incremented by 1
($i = i + 1$) at step A6. At step A7, it is determined
whether $i \leq D$. If the value i is equal to or smaller

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1 than the maximum number D of delayed samples, the
process returns to step A3. If the value i exceeds
the maximum number D of delayed samples, the process
proceeds with step A8. At step A8, it is determined
5 that the value ip is greater than the value imax. If
the answer is YES, the value ip obtained at that time
is set to imax at step A9. If the answer is NO, the
variable p is incremented by 1 ($p = p + 1$) at step
A10. At step A11 it is determined whether $p \leq n$. If
10 the answer of step A11 is YES, the process returns to
step A2. If the answer is NO, the retrieval of the
crosscorrelation function value $R_p(i)$ ends, so that
the maximum value imax of the IP within the range of i
 $\leq D$.

15 The number dp of delayed samples of the
delay unit can be obtained as follows by using the
terms ip and imax obtained by the above maximum value
detection:

$$20 \quad dp = imax - ip \quad (14)$$

Hence, the numbers di - dn of delayed samples of the
delay units 8-1 - 8-n can be set by the delay
calculator 9.

25 The filters 2-1 - 2-n can be configured as
shown in Fig. 5. When the output signals of the
filters 2-1 - 2-n are denoted as outp ($p = 1, 2, \dots,$
n) defined by the following:

$$30 \quad outp = \sum_{i=1}^n cpi * fp(i) \quad (15)$$

where $\sum_{i=1}^n$ denotes a summation from $i=1$ to $i=n$, cpi
denotes the filter coefficients, and fp(i) denotes the
values of the memories of the filters and are also
35 input signals applied to the filters.

The filter coefficient calculator 4
calculates the crosscorrelation between the present

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1 and past input signals of the filters 2-1 - 2-n and
the signals form the noise source, and thus updates
the filter coefficients. The crosscorrelation
function value $fp(i)'$ is written as follows:

$$5 \quad fp(i)' = \sum_{n=1}^q x(j) * fp(i+j-1) \quad (16)$$

where $\sum_{n=1}^q$ denotes a summation from $j=1$ to $J=q$, and
the symbol q denotes the number of samples on which
10 the convolutional operation is carried out in order to
calculate the crosscorrelation function value and is
normally equal to tens to hundreds of samples.

By using the above crosscorrelation function
value $fp(i)'$, the output signal e' of the adder 3 is
15 obtained as follows:

$$e' = \sum_{j=1}^r [f1(j)' * c1j] - \sum_{j=1}^n [fi(j)' * ci j] \quad (17)$$

20 The above operation is the convolutional operation and
can be thus implemented by a digital signal processor
(DSP). In this case, the adder 3 subtracts the output
signals of the microphones 1-2 - 1-n obtained via the
filters 2-2 - 2-n from the output signal of the
25 reference microphone 1-1 obtained via the filter 2-1.

The evaluation function is defined so that J
 $= (e')^2$ where the output signal e' of the adder 3 is
handled as an error signal. By using the evaluation
function $J = (e')^2$, the filter coefficients are
30 obtained. For example, the filter coefficients can be
obtained by the steepest descent method. By using the
following expressions, the filter coefficients $c11$,
 $c12$, ..., $cn1$, $cn2$, ..., cnr can be obtained as
follows:

35

$$\begin{bmatrix} cl1 \\ cl2 \\ \vdots \\ clr \end{bmatrix} = \begin{bmatrix} cl1_{old} \\ cl2_{old} \\ \vdots \\ clr_{old} \end{bmatrix} - t1 * \begin{bmatrix} fl(1)' \\ fl(2)' \\ \vdots \\ fl(r)' \end{bmatrix} \quad \dots (18)$$

5

$$\begin{bmatrix} cp1 \\ cp2 \\ \vdots \\ cpr \end{bmatrix} = \begin{bmatrix} cp1_{old} \\ cp2_{old} \\ \vdots \\ cpr_{old} \end{bmatrix} + tp * \begin{bmatrix} fp(1)' \\ fp(2)' \\ \vdots \\ fp(r)' \end{bmatrix} \quad \dots (19)$$

10

$$tp = \alpha * (e' / fp_{norm})$$

p=2, 3, . . . n

where the norm fp_{norm} corresponds to the
aforementioned formula (3) and can be written as
15 follows:

$$fp_{norm} = [(fp(1)')^2 + (fp(2)')^2 + \dots + (fp(r)')^2]^{1/2} \quad (20)$$

20 The term α in the equations (18) and (19) is a
constant as has been described previously, and
represents the speed and precision of convergence of
the filter coefficients towards the optimal values.

Hence, the output signal e' of the adder 3
25 is obtained as follows:

$$e' = out1 - \sum_{i=2}^n outi \quad (21)$$

The delay units 8-1 - 8-n change the phases of the
30 input signals applied to the filters 2-1 - 2-n.
Hence, the filter coefficients can easily be updated
by the filter coefficient calculator 4. Even under a
situation such that the speaker 5 speaks at the same
time as a sound is emitted from the speaker 6, the
35 updating of the filter coefficients can be realized.
Hence, it is possible to definitely suppress the noise
components that enter the microphones 1-1 - 1-n from

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1 the speaker 6 which serves as a noise source.

Fig. 8 is a block diagram of a third
embodiment of the present invention, in which parts
that are the same as those shown in Fig. 4 are given
5 the same reference numbers. In Fig. 8, there are a
noise source 16 and a supplementary microphone 21.
The supplementary microphone 21 can have the same
structure as that of the microphones 1-1 - 1-n forming
the microphone array.

10 The structure shown in Fig. 8 differs from
that shown in Fig. 4 in that the output signal of the
supplementary microphone 21 can be input to the filter
coefficient calculator 4 as a signal from the noise
source. Hence, even in a case where the noise source
15 16 is an arbitrary noise source other than the
speaker, such as an air conditioning system, the noise
can be suppressed by using the evaluation function $J = (e')^2$ used to update the filter coefficients, as has
been described with reference to Fig. 4.

20 Fig. 9 is a block diagram of a fourth
embodiment of the present invention, in which parts
that are the same as those shown in Figs. 6 and 7 are
given the same reference numbers. The structure shown
in Fig. 9 is almost the same as that shown in Fig. 6
25 except that the output signal of the supplementary
microphone 21 is applied, as the signal from a noise
source, to the delay calculator 9 and the filter
coefficient calculator 4. Hence, as in the case of
the structure shown in Fig. 6, the numbers of delayed
30 samples of the delay units 2-1 - 2-n are controlled by
the delay calculator 9, and the filter coefficients of
the filters 2-1 - 2-n are updated by the filter
coefficient calculator 4. Hence, noise can be
compressed.

35 Fig. 10 is a block diagram of a low-pass
filter used in the filter coefficient updating process
used in the embodiments of the present invention. The

1 low-pass filter shown in Fig. 10 includes coefficient
units 22 and 23, an adder 24 and a delay unit 25. The
structure shown in Fig. 10 is directed to calculating
the aforementioned crosscorrelation function value
5 $fp(i)'$ in which the coefficient unit 23 has a filter
coefficient β and the coefficient unit 22 has a filter
coefficient $(1-\beta)$. The value $fp(i)'$ is obtained as
follows:

10
$$fp(i)' = \beta * fp(i)'_{old} + (1-\beta) * [x(1) * fp(i)] \quad (22)$$

where the coefficient β is set so as to satisfy $0.0 < \beta < 1.0$ and $fp(i)'_{old}$ denotes the value of a memory (delay unit 25) of the low-pass filter.

15 The low-pass filter shown in Fig. 10 is a cyclic type low-pass filter, in which weighting for the past signals is made comparatively light in order to prevent the convolutional operation from outputting an excessive output value and thus stably obtain the crosscorrelation function value $fp(i)'$.
20

Fig. 11 is a block diagram of a structure directed to implementing the embodiments of the present invention by using a digital signal processor (DSP). Referring to Fig. 11, there are provided the
25 microphones 1-1 - 1-n forming a microphone array, a DSP 30, low-pass filters (LPF) 31-1 - 31-n, analog-to-digital (A/D) converters 32-1 - 32-n, a digital-to-analog (D/A) converter 33, a low-pass filter (LPF) 34, an amplifier 35 and a speaker 36.

30 The aforementioned filters 2-1 - 2-n and the filter coefficient calculator 4 used in the structure shown in Fig. 4 and the filters 2-1 - 2-n, the filter coefficient calculator 4 and the delay units 8-1 - 8-n used in the structure shown in Fig. 6 can be realized
35 by the combinations of a repetitive process, a sum-of-product operation and a condition branching process. Hence, the above processes can be implemented by

1 operating functions of the DSP 30.

The low-pass filters 31-1 - 31-n function to eliminate signal components located outside the speech band. The A/D converters 32-1 - 32-n converts the
5 output signals of the microphones 1-1 - 1-n obtained via the low-pass filters 31-1 - 31-n into digital signals and have a sampling frequency of, for example, 8 kHz. The digital signals have the number of bits which corresponds to the number of bits processed in
10 the DSP 30. For example, the digital signals consists of 8 bits or 16 bits.

An input signal obtained via a network or the like is converted into an analog signal by the D/A converter 33. The analog signal thus obtained passes
15 through the low-pass filter 34, and is then applied to the amplifier 35. An amplified signal drives the speaker 36. The reproduced sound emitted from the speaker 36 serves as noise with respect to the microphones 1-1 - 1-n. However, as has been described
20 previously, the noise can be suppressed by updating the filter coefficients by the DSP 30.

Fig. 12 is a block diagram showing functions of the DSP that can be used in the embodiments of the present invention. In Fig. 12, parts that are the
25 same as those shown in the previously described figures are given the same reference numbers. In Fig. 12, the low-pass filters 31-1 - 31-n and 34, the A/D converters 32-1 - 32-n, the D/A converter 33 and the amplifier 35 shown in Fig. 11 are omitted. The filter
30 coefficient calculator 4 includes a crosscorrelation calculator 41 and a filter coefficient updating unit 42. The delay calculator 9 includes a crosscorrelation calculator 43, a maximum value detector 44 and a number-of-delayed-samples calculator
35 45.

The crosscorrelation calculator 43 of the delay calculator 9 receives the output signals $gp(j9$

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1 of the microphones 1-1 - 1-n and the drive signal for
the speaker 36 (which functions as a noise source),
and calculates the crosscorrelation function value
Rp(i) defined in formula (13). The maximum value
5 detector 44 detects the maximum value of the
crosscorrelation function value Rp(i) in accordance
with the flowchart of Fig. 7. The number-of-delayed-
samples calculator 45 obtain the numbers dp of delayed
samples of the delay units 8-1 - 8-n by using the ip
10 and imax obtained during the maximum value detecting
process. The numbers of delayed samples thus obtained
are then set in the delay units 8-1 - 8-n.

The crosscorrelation calculator 41 of the
filter coefficient calculator 4 receives the signals
15 from the noise source delayed so that these signals
are in phase by the delay units 8-1 - 8-n, the drive
signal for the speaker 36 serving as a noise source,
and the output signal of the adder 3, and calculates
the crosscorrelation function value fp(i)' in
20 accordance with equation (16). In the process of
calculating the crosscorrelation function value
fp(i)', the low-pass filtering process shown in Fig.
10 can be included. The filter coefficient updating
unit 42 calculates the filter coefficients cpr in
25 accordance with the equations (17), (18) and (19), and
thus the filter coefficients of the filters 2-1 - 2-n
shown in Fig. 5 can be updated.

Fig. 13 is a block diagram of a structure of
the delay units. Each delay unit includes a memory
30 46, a write controller 47, and a read controller 49,
which controllers are controlled by the delay
calculator 9. The delay unit shown in Fig. 13 is
implemented by an internal memory built in the DSP.
The memory 46 has an area corresponding to the maximum
35 value D of delayed samples. The write operation is
performed under the control of the write controller
47, and the read operation is performed under the

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1 control of the read controller 48. A write pointer WP
and a read pointer RP are set at intervals equal to
the number dp of delayed samples calculated by the
calculator 9. Further, the write pointer WP and the
5 read pointer RP are shifted in the directions
indicated by arrows of broken lines at every
write/read timing. Hence, the signal written into the
address indicated by the write pointer WP is read when
it is indicated by the read pointer RP after the
10 number dp of delayed samples.

Fig. 14 is a block diagram of a fifth
embodiment of the present invention, which includes
microphones 51-1 and 51-2 forming a microphone array,
linear predictive filters 52-1 and 52-2, liner
15 predictive analysis units 53-1 and 53-2, a sound
source position detector 54 and a sound source 55 such
as a speaker. Although a plurality of microphones
more than two can be used to form a microphone array,
the structure uses only two microphones 51-1 and 51-2
20 for the sake of simplicity.

The output signals $a(j)$ and $b(j)$ of the
microphones 51-1 and 51-2 are applied to the linear
predictive analysis units 53-1 and 53-2 and the linear
predictive filters 52-1 and 52-2. Then, the linear
25 predictive analysis units 53-1 and 53-2 obtain
autocorrelation function value and thus calculate
linear predictive coefficients, which are used to
update the filter coefficients of the linear
predictive filters 52-1 and 52-2. Then, the position
30 of the sound source 55 is detected by the sound source
detector 54 by using a linear predictive residual
signal which is the difference between the output
signals of the linear predictive filters 52-1 and 52-
2. Finally, information concerning the position of
35 the sound source is output.

Fig. 15 is a block diagram of the internal
structures of the blocks shown in Fig. 14. Referring

1 to Fig. 15, there are illustrated autocorrelation
function value calculators 56-1 and 56-2, linear
predictive coefficient calculators 57-1 and 57-2, a
crosscorrelation coefficient calculator 58, and a
5 position detection processing unit 59. The linear
predictive analysis units 53-1 and 53-2 include the
autocorrelation function value calculators 56-1 and
56-2, and the linear predictive coefficient
calculators 57-1 and 57-2, respectively. The output
10 signals a(j) and b(j) of the microphones 51-1 and 51-2
are respectively input to the autocorrelation function
value calculators 56-1 and 56-2.

The autocorrelation function value
calculator 56-1 of the linear predictive analysis unit
15 53-1 calculates the autocorrelation function value
 $R_a(i)$ by using the output signal a(i) of the
microphone 51-1 and the following formula:

$$R_a(i) = \sum_{j=1}^n a(j) * a(j+i) \quad (23)$$

20 where $\sum_{j=1}^n$ denotes a summation of $j=1$ to $j=n$, and the
symbol n denotes the number of samples on which the
convolutional operation is carried out and is
generally equal to a few of hundreds. When the symbol
25 q denotes the order of the linear predictive filter,
then $0 \leq i \leq q$.

The linear predictive coefficient calculator
57-1 calculates the linear predictive coefficients
 $\alpha a_1, \alpha a_2, \dots, \alpha a_q$ on the basis of the autocorrelation
30 function value $R_a(i)$. The linear predictive
coefficients can be obtained any of various known
methods such as an autocorrelation method, a partial
correlation method and a covariance method. Hence,
the linear predictive coefficients can be implemented
35 by the operational functions of the DSP.

In the linear predictive analysis unit 53-2
corresponding to the microphone 51-2, the

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- 1 autocorrelation function value calculator 56-2
calculates the autocorrelation function value $R_b(i)$ by
using the output signal $b(j)$ of the microphone 51-2 in
the same manner as the formula (23). The linear
5 predictive coefficient calculator 57-2 calculates the
linear predictive coefficients ab_1, ab_2, \dots, ab_q .

The linear predictive filters 52-1 and 52-2
may have an q th-order FIR filter. Hence, the filter
coefficients c_1, c_2, \dots, c_q are respectively updated
10 by the linear predictive coefficients $aa_1, aa_2, \dots,$
 $aa_q, ab_1, ab_2, \dots, ab_q$. The filter order q of the
linear predictive filters 52-1 and 52-2 is defined by
the following expression:

$$15 \quad q = [(\text{sampling frequency}) * (\text{intermicrophone distance})] / (\text{speed of sound}) \quad (24)$$

The high-hand side of the formula (24) is the same as
that of the aforementioned formula (7).

- 20 The source position detector 54 includes the
crosscorrelation coefficient calculator 58 and the
position detection processing unit 59. The
crosscorrelation coefficient calculator 58 calculates
the crosscorrelation coefficient $r'(i)$ by using the
25 output signals of the linear predictive filters 52-1
and 52-2, that is, the linear predictive residual
signals $a'(j)$ and $b'(j)$ for the output signals $a(j)$
and $b(j)$ of the microphones 51-1 and 51-2. In this
case, the variable i meets $-q \leq i \leq q$.

- 30 The position detection processing unit 59
obtains the value of i at which the crosscorrelation
coefficient $r'(i)$ is maximized, and outputs sound
source position information indicative of the position
of the sound source 55. The relation between the
35 sound source position and the i_{\max} is as shown in Fig.
16. When $i_{\max} = 0$, the sound source 55 is located in
front of or at the back of the microphones 51-1 and

1 51-2, and is spaced apart from the microphones 51-1
and 51-2 by an even distance. When $imax = q$, the
sound source 55 is located on an imaginary line
connecting the microphones 51-1 and 51-2 and is closer
5 to the microphone 51-1. When $imax = -q$, the sound
source 55 is located on an imaginary line connecting
the microphones 51-1 and 51-2 and is closer to the
microphone 51-2. If three or more microphones are
used, it is possible to detect the position of the
10 sound source including information indicating the
distances to the sound source.

Generally, the speech signal has a
comparatively large autocorrelation function value.
The prior art directed to obtaining the
15 crosscorrelation function $r(i)$ using the output
signals $a(j)$ and $b(j)$ of the microphones 51-1 and 51-2
cannot easily detect the position of the sound source
because the crosscorrelation coefficient $r(i)$ does not
change greatly as a function of the variable i . In
20 contrast, according to the embodiments of the present
invention, the position of the sound source can be
easily detected even for a large autocorrelation
function value because the crosscorrelation
coefficient $r'(i)$ is obtained by using the linear
25 predictive residual signals.

Fig. 17 is a block diagram of a sixth
embodiment of the present invention, in which parts
that are the same as those shown in Fig. 14 are given
the same reference numbers. Referring to Fig. 17,
30 there are illustrated a linear predictive analysis
unit 53A and a speaker 55A serving as a sound source.1
A drive signal for the speaker 55A is applied to the
linear predictive analysis unit 53A, which analyzes
the signal of the sound source in the linear
35 predictive manner, and thus obtain the linear
predictive coefficients. The linear predictive
analysis unit 53 is provided in common to the linear

1 predictive filters 52-1 and 52-2. The linear
predictive residual signals for the output signals
a(j) and b(j) of the microphones 51-1 and 51-2 are
obtained. The sound source position detecting unit 54
5 obtains the crosscorrelation coefficient $r'(i)$ by
using the obtained linear predictive residual signals.
Hence, the position of the sound source can be
identified.

Fig. 18 is a block diagram of a seventh
10 embodiment of the present invention. Referring to
Fig. 18, there are illustrated microphones 61-1 and
61-2 forming a microphone array, a signal estimator
62, a synchronous adder 63, and a sound source 65.
The synchronous adder 63 performs a synchronous
15 addition operation on the output signals of the
microphones 61-1 and 61-2 assuming that microphones
64-1, 64-2, ... are present at estimated positions
depicted by the broken lines, these estimated
positions being located on an imaginary line
20 connecting the microphones 61-1 and 61-2 together.

Fig. 19 is a block diagram of the detail of
the seventh embodiment of the present invention, in
which parts that are the same as those shown in Fig.
18 are given the same reference numbers. There are
25 provided a particle velocity calculator 66, an
estimation processing unit 67, delay units 68-1, 68-
2, ..., and an adder 69. Fig. 19 shows a case where
the sound source 65 is located at an angle θ with
respect to the imaginary line connecting the
30 microphones 61-1 and 61-2 forming the microphone
array. The process is carried out under an assumption
that the microphones 64-1, 64-2, ... are arranged on
the imaginary line as depicted by the symbols of
broken lines.

35 The signal estimator 62 includes the
particle velocity calculator 66 and the estimation
processing unit 67. A propagation of the acoustic

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1 wave from the sound source 65 can be expressed by the
wave equation as follows:

$$\begin{aligned} -\partial V / \partial x &= (1/K)(\partial P / \partial t) \\ 5 \quad -\partial P / \partial t &= \sigma(\partial V / \partial t) \end{aligned} \quad (25)$$

where P is the sound pressure, V is the particle velocity, K is the bulk modulus, and σ is the density of a medium.

10 The particle velocity calculator 66 calculates the velocity of particles from the difference between a sound pressure P(j, 0) corresponding to the amplitude of the output signal a(j) of the microphone 61-1 and a sound pressure P(j, 1) corresponding to the amplitude of the output signal b(j) of the microphone 61-2. That is, the velocity V(j+1, 0) of particles at the microphone 61-1 is as follows:

$$20 \quad V(j+1, 0) = V(j, 0) + [P(j, 1) - P(j, 0)] \quad (26)$$

where j is the sample number.

The estimation processing unit 67 obtains estimated positions of the microphones 64-1, 64-2, ...
25 by the following equations:

$$\begin{aligned} P(j, x+1) &= P(j, x) + \beta(x)[V(j+1, x) - V(j, x)] \\ V(j+1, x) &= V(j+1, x-1) + [P(j, x-1) - P(j, x)] \end{aligned} \quad (27)$$

30 where x denotes an estimated position and $\beta(x)$ is an estimation coefficient.

If the positions of the microphones 61-2 and 61-1 are described so that $x = 1$ and $x = 0$, respectively, the microphones 64-1 and 64-2 are respectively located at estimated positions of $x = 2$ and $x = 3$. The estimation processing unit 62 supplies, by using the two microphones 61-1 and 61-2,

1 the synchronous adder 63 with the output signals of
the microphones 64-1, 64-2, ..., as if these
microphones 64-1, 64-2, ... are actually arranged.
Hence, even the microphone array formed by only the
5 two microphones 61-1 and 61-2 can emphasize the target
sound by the synchronous adding operation as if a
large number of microphones is arranged.

The synchronous adder 63 includes the delay
units 68-1, 68-2, ..., and the adder 69. When the
10 number of delayed samples is denoted as d , the delay
units 68-1, 68-2, ... can be described as z^{-d} , z^{-2d} ,
 z^{-3d} , The number d of delayed samples is
calculated as follows by using the angle θ with
respect to the imaginary line connecting the
15 microphones 61-1 and 61-2 together obtained by the
aforementioned manner:

$$d = \frac{[(\text{number of sampling frequency}) * (\text{intermicrophone distance}) * \cos \theta]}{(\text{velocity of sound})} \quad (28)$$

20

Hence, the output signals of the microphones
61-1 and 61-2 and the output signals of the
microphones 64-1, 64-2, ... located at estimated
25 positions are pulled in phase by the delay units 68-1,
68-2, ..., and are then added by the adder 69. Hence,
the target sound can be emphasized by the synchronous
addition operation. With the above arrangement, the
target sound can be emphasized so as to have a power
30 obtained by a small number of actual microphones and
the estimated microphones.

Fig. 20 is a block diagram of an eighth
embodiment of the present invention in which parts
that are the same as those shown in Fig. 18 are given
35 the same reference numbers. Provided are a reference
microphone 71, a subtracter 72, a weighting filter 73
and an estimation coefficient decision unit 74. In

1 the eight embodiment of the present invention, the
reference microphone 71 is arranged at a position of x
= 2 so as to have the same intervals as those at which
the microphone 61-1 and the microphone 61-2 are
5 located at positions of $x = 0$ and $x = 1$. An estimated
position error is obtained by the subtracter 72. The
weighting filter 73 processes the estimated position
error so as to have an acoustic sense characteristic.
Then, the estimation coefficient decision unit 74
10 determines the estimation coefficient $\beta(x)$.

More particularly, the subtracter 72
calculates an estimation error $e(j)$ which is the
difference between the estimated signal $(j,2)$ of the
microphone 64-1 located at $x = 2$ and the output signal
15 $ref(j)$ of the reference microphone 71 by the following
formula:

$$\begin{aligned} e(j) &= P(j,2) - ref(j) \\ &= P(j,1) + \beta(2)[V(j+1,1) - V(j,1)] - ref(j) \end{aligned} \quad (29)$$

20

The estimation coefficient decision unit 74
can determine the estimation coefficient $\beta(2)$ so that
the average power of the estimation error $e(j)$ can be
25 minimized. That is, the estimation processing unit 62
(shown in Fig. 18 or Fig. 19) performs an estimation
process for the output signals of the estimated
microphones 64-1, 64-2, ... by using the estimation
coefficient $\beta(2)$ with $x = 2, 3, 4, \dots$, and outputs
30 the operation result.

The weighting filter 73 weights the
estimation error $e(j)$ in accordance with the acoustic
sense characteristic, which is known a loudness
characteristic in which sensitivity obtained around 4
35 kHz is comparatively high. More particularly, a
comparatively large weight is given to frequency
components of the estimation error $e(j)$ around 4 kHz.

1 Hence, even in the process for the estimated
microphones located at $x = 2, 3, \dots$, the estimation
error can be reduced in the band having comparatively
high sensitivity, and the target sound can be
5 emphasized by the synchronous adding operation.

Fig. 21 is a block diagram of a ninth
embodiment of the present invention. The structure
shown in Fig. 21 includes the microphones 61-1 and 61-
2 forming a microphone array, signal estimators 62-1,
10 62-2, ..., 62-s, synchronous adders 63-1, 63-2, ...,
63-n, estimated microphones 64-1, 64-2, ..., the sound
source 65, and a sound source position detector 80.

The angles $\theta_0, \theta_1, \dots, \theta_s$ are defined with
respect to the microphone array of the microphones 61-
15 1 and 61-2, and the signal estimators 62-1 - 62-s and
the synchronous adders 63-1 - 63-s are provided to the
respective angles. The signal estimators 62-1 - 62-s
obtain estimated coefficients $\beta(x, \theta)$ beforehand. For
example, as shown in Fig. 20, the reference microphone
20 71 is provided to obtain the estimated coefficient
 $\beta(x, \theta)$.

The synchronous adders 63-1 - 63-s pull the
output signals of the signal estimators 62-1 - 62-s in
phase, and add these signals. Hence, the output
25 signals corresponding to the angles $\theta_0 - \theta_s$ can be
obtained. The sound source position detector 80
compares the output signals of the synchronous adders
63-1 - 63-s with each other, and determines that the
angle at which the maximum power can be obtained is
30 the direction in which the sound source 65 is located.
Then, the detector 80 outputs information indicating
the position of the sound source. Further, the
detector 80 can output the signal having the maximum
power as the emphasized target signal.

35 Fig. 22 is a block diagram of a tenth
embodiment of the present invention, which includes a
camera such as a video camera or a digital camera,

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1 microphones 91-1 and 91-2 forming a microphone array,
a sound source detector 92, a face position detector
93, an integrate decision processing unit 94 and a
sound source 95.

5 The microphones 91-1 and 91-2 and the sound
source position detector 92 is any of those used in
the aforementioned embodiments of the present
invention. The information concerning the position of
the sound source 95 is applied to the integrate
10 decision processing unit 94 by the sound source
position detector 92. The position of the face of the
speaker is detected from an image of the speaker taken
by the camera 90. For example, a template matching
method using face templates may be used. An
15 alternative method is to extract an area having skin
color from a color video signal. The integrate
decision processing unit 94 detects the position of
the sound source 95 based on the position information
from the sound source position detector 92 and the
20 position detection information from the face position
detector 93.

For example, a plurality of angles $\theta_0 - \theta_s$
are defined with respect to the imaginary line
connecting the microphones 91-1 and 91-2 and the
25 picture taking direction of the camera 90. Then,
position information $\text{inf-A}(\theta)$ indicating the
probability of the direction in which the sound source
95 may be located is obtained by a sound source
position detecting method for calculating the
30 crosscorrelation coefficient based on the linear
predictive errors of the output signals of the
microphones 91-1 and 91-2 or by another method using
the output signals of the real microphones 91-1 and
91-2 and estimated microphones located on the
35 imaginary line connecting the microphones 91-1 and 91-
2 together. Also, position information $\text{inf-V}(\theta)$
indicating the probability of the direction in which

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1 the face of the speaker may be located is obtained.
Then, the integrate decision processing unit 94
calculates the product $\text{res}(\theta)$ of the position
information $\text{inf-A}(\theta)$ and $\text{inf-V}(\theta)$, and outputs the
5 angle θ at which the product $\text{res}(\theta)$ is maximized as
sound source position information. Hence, it is
possible to more precisely detect the direction in
which the sound source 95 is located. It is also
possible to obtain an enlarged image of the sound
10 source 95 by an automatic control of the camera such
as a zoom-in mode.

The present invention is not limited to the
specifically disclosed embodiments, and variations and
modifications may be made without departing from the
15 scope of the present invention. For example, any of
the embodiments of the present invention can be
combined for a specific purpose such as noise
compression, target sound emphasis or sound source
position detection. The target sound emphasis and the
20 sound source position detection may be applied to not
only a speaking person but also a source emitting an
acoustic wave.

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